Low Noise, Precision Operational Amplifier

OP27

FEATURES

Low noise: 80 nV p-p (0.1 Hz to 10 Hz), 3 nV/√Hz
Low drift: 0.2 µV/°C
High speed: 2.8 V/µs slew rate, 8 MHz gain bandwidth
Low V_{OS}: 10 µV
Excellent CMRR: 126 dB at VCM of ±11 V
High open-loop gain: 1.8 million
Fits 725, OP07, 5534A sockets
Available in die form

GENERAL DESCRIPTION

The OP27 precision operational amplifier combines the low offset and drift of the OP07 with both high speed and low noise. Offsets down to 25 µV and maximum drift of 0.6 µV/°C make the OP27 ideal for precision instrumentation applications. Exceptionally low noise, e_n = 3.5 nV/√Hz, at 10 Hz, a low 1/f noise corner frequency of 2.7 Hz, and high gain (1.8 million), allow accurate high-gain amplification of low-level signals. A gain-bandwidth product of 8 MHz and a 2.8 V/µs slew rate provides excellent dynamic accuracy in high speed, data-acquisition systems.

A low input bias current of ±10 nA is achieved by use of a bias-current-cancellation circuit. Over the military temperature range, this circuit typically holds IB and IOS to ±20 nA and 15 nA, respectively.

The output stage has good load driving capability. A guaranteed swing of ±10 V into 600 Ω and low output distortion make the OP27 an excellent choice for professional audio applications.

(Continued on Page 3)

PIN CONNECTIONS

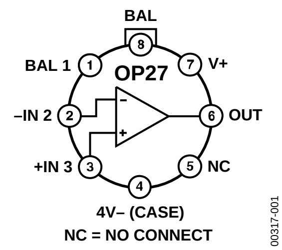

Figure 1. TO-99 (J-Suffix)

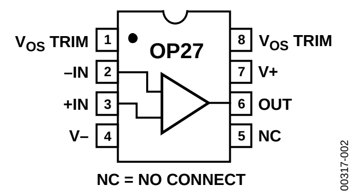

Figure 2. 8-Lead Hermetic DIP (Z-Suffix) 8-Lead Plastic DIP (P-Suffix) 8-Lead SO (S-Suffix)

SIMPLIFIED SCHEMATIC

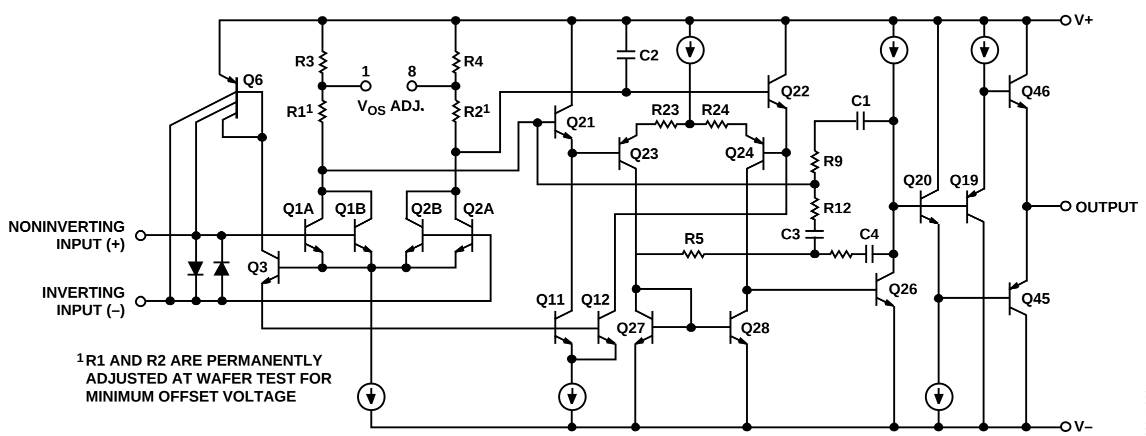

Figure 3.

Rev. E

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TABLE OF CONTENTS

REVISION HISTORY

12/05—Rev. D to Rev. E
Edits to Figure 2 1

9/05—Rev. C to Rev. D
Updated Format .... Universal
Changes to Table 1 4
Removed Die Characteristics Figure 5
Removed Wafer Test Limits Table 5
Changes to Table 5 7
Changes to Comments on Noise Section 15
Changes to Ordering Guide 24

1/03—Rev. B to Rev. C
Edits to Pin Connections 1
Edits to General Description 1
Edits to Die Characteristics 5
Edits to Absolute Maximum Ratings 7
Updated Outline Dimensions 16
Edits to Figure 8 14
Edits to Outline Dimensions 16

9/01—Rev. 0 to Rev. A
Edits to Ordering Information 1
Edits to Pin Connections 1
Edits to Absolute Maximum Ratings 2
Edits to Package Type 2
Edits to Electrical Characteristics 2, 3
Edits to Wafer Test Limits 4
Deleted Typical Electrical Characteristics 4
Edits to Burn-In Circuit Figure 7
Edits to Application Information 8

GENERAL DESCRIPTION

(continued from Page 1)

PSRR and CMRR exceed 120 dB. These characteristics, coupled with long-term drift of 0.2 μV/month, allow the circuit designer to achieve performance levels previously attained only by discrete designs.

Low cost, high volume production of OP27 is achieved by using an on-chip Zener zap-trimming network. This reliable and stable offset trimming scheme has proved its effectiveness over many years of production history.

The OP27 provides excellent performance in low noise, high accuracy amplification of low level signals. Applications include stable integrators, precision summing amplifiers, precision voltage threshold detectors, comparators, and professional audio circuits such as tape-heads and microphone preamplifiers.

The OP27 is a direct replacement for 725, OP06, OP07, and OP45 amplifiers; 741 types may be directly replaced by removing the 741's nulling potentiometer.

SPECIFICATIONS

ELECTRICAL CHARACTERISTICS

$V_S = \pm15$ V, $T_A = 25°C$, unless otherwise noted.

Table 1.

			OP27A/E			OP27/G			
Parameter	**Symbol**	**Conditions**	**Min**	**Typ**	**Max**	**Min**	**Typ**	**Max**	**Unit**
INPUT OFFSET VOLTAGE[1]	V_{OS}			10	25		30	100	µV
LONG-TERM V_{OS} STABILITY[2, 3]	V_{OS}/Time			0.2	1.0		0.4	2.0	µV/M_O
INPUT OFFSET CURRENT	I_{OS}			7	35		12	75	nA
INPUT BIAS CURRENT	I_B			±10	±40		±15	±80	nA
INPUT NOISE VOLTAGE[3, 4]	$e_{n\ p\text{-}p}$	0.1 Hz to 10 Hz		0.08	0.18		0.09	0.25	µV p-p
INPUT NOISE Voltage Density[3]	e_n	f_O = 10 Hz		3.5	5.5		3.8	8.0	nV/√Hz
		f_O = 30 Hz		3.1	4.5		3.3	5.6	nV/√Hz
		f_O = 1000 Hz		3.0	3.8		3.2	4.5	nV/√Hz
INPUT NOISE Current Density[3]	i_n	f_O = 10 Hz		1.7	4.0		1.7		pA/√Hz
		f_O = 30 Hz		1.0	2.3		1.0		pA/√Hz
		f_O = 1000 Hz		0.4	0.6		0.4	0.6	pA/√Hz
INPUT RESISTANCE									
Differential Mode[5]	R_{IN}		1.3	6		0.7	4		MΩ
Common Mode	R_{INCM}			3			2		GΩ
INPUT VOLTAGE RANGE	IVR		±11.0	±12.3		±11.0	±12.3		V
COMMON-MODE REJECTION RATIO	CMRR	V_{CM} = ±11 V	114	126		100	120		dB
POWER SUPPLY REJECTION RATIO	PSRR	V_S = ±4 V to ±18 V		1	10		2	20	µV/V
LARGE-SIGNAL VOLTAGE GAIN	A_{VO}	R_L ≥ 2 k Ω, V_O = ±10 V	1000	1800		700	1500		V/µV
		R_L ≥ 600 Ω, V_O = ±10 V	800	1500		600	1500		V/µV
OUTPUT VOLTAGE SWING	V_O	R_L ≥ 2 k Ω	±12.0	±13.8		±11.5	±13.5		V
		R_L ≥ 600 Ω	±10.0	±11.5		±10.0	±11.5		V
SLEW RATE[6]	SR	R_L ≥ 2 kΩ	1.7	2.8		1.7	2.8		V/µs
GAIN BANDWIDTH PRODUCT[6]	GBW		5.0	8.0		5.0	8.0		MHz
OPEN-LOOP OUTPUT RESISTANCE	R_O	V_O = 0, I_O = 0		70			70		Ω
POWER CONSUMPTION	P_d	V_O		90	140		100	170	mW
OFFSET ADJUSTMENT RANGE		R_P = 10 kΩ		±4.0			±4.0		mV

[1] Input offset voltage measurements are performed ~ 0.5 seconds after application of power. A/E grades guaranteed fully warmed up.
[2] Long-term input offset voltage stability refers to the average trend line of V_{OS} vs. Time over extended periods after the first 30 days of operation. Excluding the initial hour of operation, changes in V_{OS} during the first 30 days are typically 2.5 µV. Refer to Typical Performance Characteristics.
[3] Sample tested.
[4] See voltage noise test circuit (Figure 31).
[5] Guaranteed by input bias current.
[6] Guaranteed by design.

V_S = ±15 V, −55°C ≤ T_A ≤ 125°C, unless otherwise noted.

Table 2.

Parameter	Symbol	Conditions	OP27A Min	OP27A Typ	OP27A Max	Unit
INPUT OFFSET VOLTAGE[1]	V_{OS}			30	60	μV
AVERAGE INPUT OFFSET DRIFT	TCV_{OS}[2]					
	TCV_{OSn}[3]			0.2	0.6	μV/°C
INPUT OFFSET CURRENT	I_{OS}			15	50	nA
INPUT BIAS CURRENT	IB			±20	±60	nA
INPUT VOLTAGE RANGE	IVR		±10.3	±11.5		V
COMMON-MODE REJECTION RATIO	CMRR	V_{CM} = ±10 V	108	122		dB
POWER SUPPLY REJECTION RATIO	PSRR	V_S = ±4.5 V to ±18 V		2	16	μV/V
LARGE-SIGNAL VOLTAGE GAIN	A_{VO}	R_L ≥ 2 kΩ, V_O = ±10 V	600	1200		V/mV
OUTPUT VOLTAGE SWING	V_O	R_L ≥ 2 kΩ	±11.5	±13.5		V

[1] Input offset voltage measurements are performed by automated test equipment approximately 0.5 seconds after application of power. A/E grades guaranteed fully warmed up.
[2] The TCV_{OS} performance is within the specifications unnulled or when nulled with R_P = 8 kΩ to 20 kΩ. TCV_{OS} is 100% tested for A/E grades, sample tested for G grades.
[3] Guaranteed by design.

V_S = ±15 V, −25°C ≤ T_A ≤ 85°C for OP27J, OP27Z, 0°C ≤ T_A ≤ 70°C for OP27EP, and −40°C ≤ T_A ≤ 85°C for OP27GP, OP27GS, unless otherwise noted.

Table 3.

Parameter	Symbol	Conditions	OP27E Min	OP27E Typ	OP27E Max	OP27G Min	OP27G Typ	OP27G Max	Unit
INPUT ONSET VOLTAGE	V_{OS}			20	50		55	220	μV
AVERAGE INPUT OFFSET DRIFT	TCV_{OS}[1]			0.2	0.6		0 4	1.8	μV/°C
	TCV_{OSn}[2]			0.2	0.6		0 4	1.8	μV/°C
INPUT OFFSET CURRENT	I_{OS}			10	50		20	135	nA
INPUT BIAS CURRENT	I_B			±14	±60		±25	±150	nA
INPUT VOLTAGE RANGE	IVR		±10.5	±11.8		±10.5	±11.8		V
COMMON-MODE REJECTION RATIO	CMRR	V_{CM} = ±10 V	110	124		96	118		dB
POWER SUPPLY REJECTION RATIO	PSRR	V_S = ±4.5 V to ±18 V		2	15		2	32	μV/V
LARGE-SIGNAL VOLTAGE GAIN	A_{VO}	R_L ≥ 2 kΩ, V_O = ±10 V	750	1500		450	1000		V/mV
OUTPUT VOLTAGE SWING	V_O	R_L ≥ 2 kΩ	±11.7	±13.6		±11.0	±13.3		V

[1] The TCV_{OS} performance is within the specifications unnulled or when nulled with R_P = 8 kΩ to 20 kΩ. TCV_{OS} is 100% tested for A/E grades, sample tested for C/G grades.
[2] Guaranteed by design.

TYPICAL ELECTRICAL CHARACTERISTICS

V_S = ±15 V, T_A = 25°C unless otherwise noted.

Table 4.

Parameter	Symbol	Conditions	OP27N Typical	Unit
AVERAGE INPUT OFFSET VOLTAGE DRIFT[1]	TCV_{OS} or TCV_{OSn}	Nulled or unnulled R_P = 8 kΩ to 20 kΩ	0.2	μV/°C
AVERAGE INPUT OFFSET CURRENT DRIFT	TCI_{OS}		80	pA/°C
AVERAGE INPUT BIAS CURRENT DRIFT	TCI_B		100	pA/°C
INPUT NOISE VOLTAGE DENSITY	e_n e_n e_n	f_O = 10 Hz f_O = 30 Hz f_O = 1000 Hz	3.5 3.1 3.0	nV/√Hz nV/√Hz nV/√Hz
INPUT NOISE CURRENT DENSITY	i_n i_n i_n	f_O = 10 Hz f_O = 30 Hz f_O = 1000 Hz	1.7 1.0 0.4	pA/√Hz pA/√Hz pA/√Hz
INPUT NOISE VOLTAGE SLEW RATE	e_{np-p} SR	0.1 Hz to 10 Hz R_L ≥ 2 kΩ	0.08 2.8	μV p-p V/μs
GAIN BANDWIDTH PRODUCT	GBW		8	MHz

[1] Input offset voltage measurements are performed by automated test equipment approximately 0.5 sec after application of power.

ABSOLUTE MAXIMUM RATINGS

Table 5.

Parameter	Rating
Supply Voltage	±22 V
Input Voltage[1]	±22 V
Output Short-Circuit Duration	Indefinite
Differential Input Voltage[2]	±0.7 V
Differential Input Current[2]	±25 mA
Storage Temperature Range	−65°C to +150°C
Operating Temperature Range	
OP27A (J, Z)	−55°C to +125°C
OP27E, (Z)	−25°C to +85°C
OP27E, (P)	0°C to 70°C
OP27G (P, S, J, Z)	−40°C to +85°C
Lead Temperature Range (Soldering, 60 sec)	300°C
Junction Temperature	−65°C to +150°C

[1] For supply voltages less than ±22 V, the absolute maximum input voltage is equal to the supply voltage.
[2] The OP27's inputs are protected by back-to-back diodes. Current limiting resistors are not used in order to achieve low noise. If differential input voltage exceeds ±0.7 V, the input current should be limited to 25 mA.

Stresses above those listed under Absolute Maximum Ratings may cause permanent damage to the device. This is a stress rating only; functional operation of the device at these or any other conditions above those indicated in the operational section of this specification is not implied. Exposure to absolute maximum rating conditions for extended periods may affect device reliability.

Absolute Maximum Ratings apply to both DICE and packaged parts, unless otherwise noted.

Table 6.

Package Type	θ_{JA}[1]	θ_{JC}	Unit
TO-99 (J)	150	18	°C/W
8-Lead Hermetic DIP (Z)	148	16	°C/W
8-Lead Plastic DIP (P)	103	43	°C/W
8-Lead SO (S)	158	43	°C/W

[1] θ_{JA} is specified for worst-case mounting conditions, that is, θ_{JA} is specified for device in socket for TO, CERDIP, and P-DIP packages; θ_{JA} is specified for device soldered to printed circuit board for SO package.

ESD CAUTION

ESD (electrostatic discharge) sensitive device. Electrostatic charges as high as 4000 V readily accumulate on the human body and test equipment and can discharge without detection. Although this product features proprietary ESD protection circuitry, permanent damage may occur on devices subjected to high energy electrostatic discharges. Therefore, proper ESD precautions are recommended to avoid performance degradation or loss of functionality.

TYPICAL PERFORMANCE CHARACTERISTICS

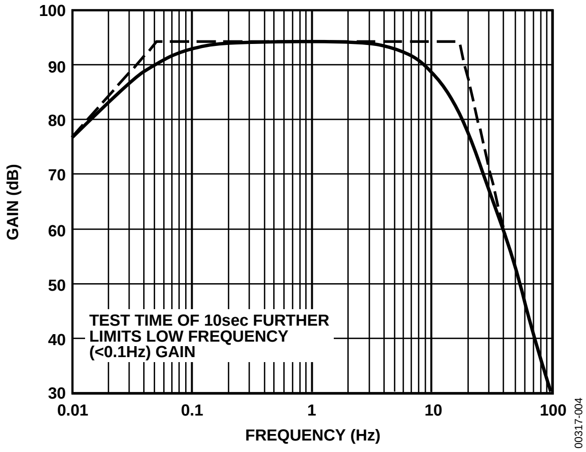

Figure 4. 0.1 Hz to 10 Hz_{p-p} Noise Tester Frequency Response

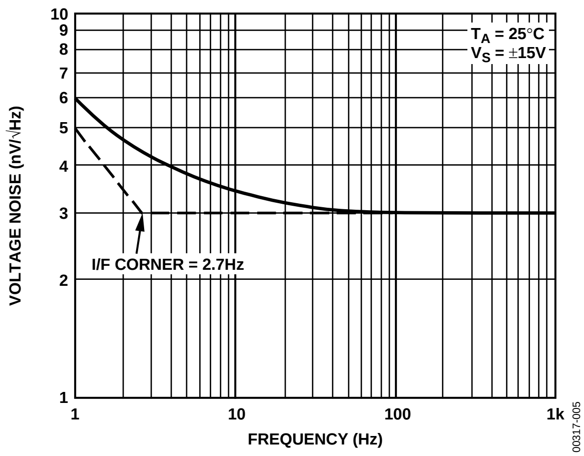

Figure 5. Voltage Noise Density vs. Frequency

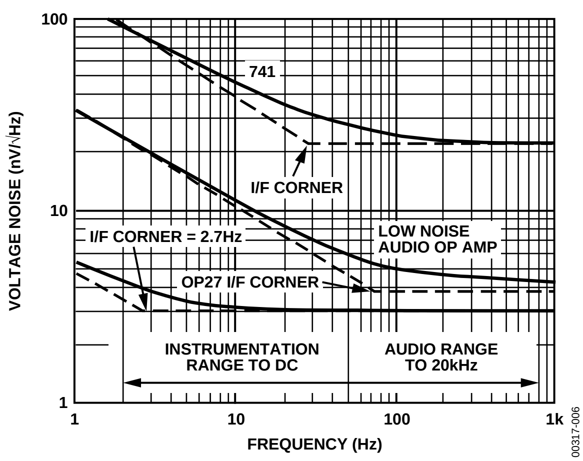

Figure 6. A Comparison of Op Amp Voltage Noise Spectra

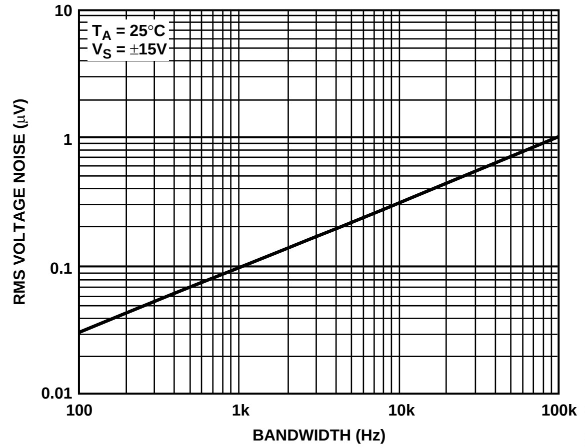

Figure 7. Input Wideband Voltage Noise vs. Bandwidth (0.1 Hz to Frequency Indicated)

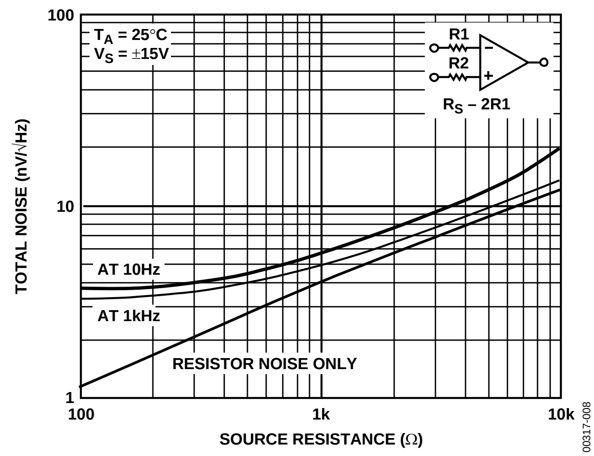

Figure 8. Total Noise vs. Sourced Resistance

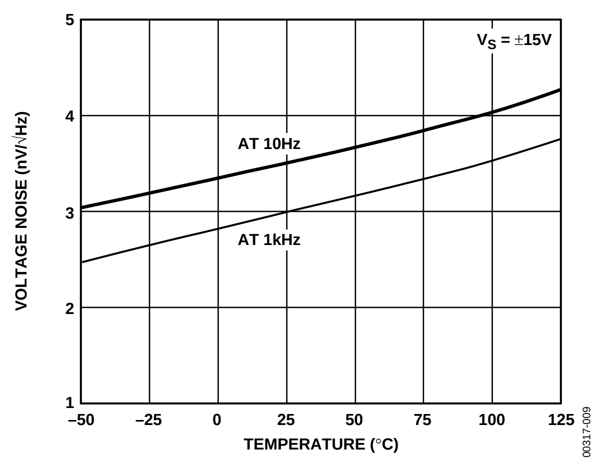

Figure 9. Voltage Noise Density vs. Temperature

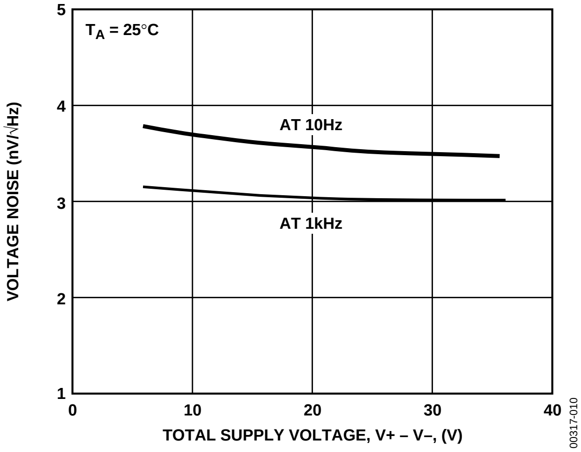

Figure 10. Voltage Noise Density vs. Supply Voltage

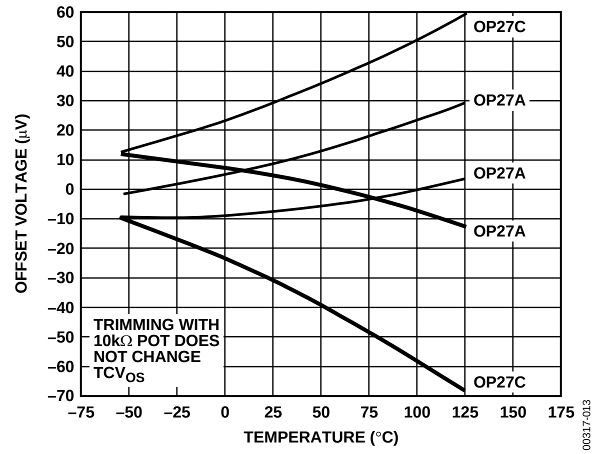

Figure 13. Offset Voltage Drift of Five Representative Units vs. Temperature

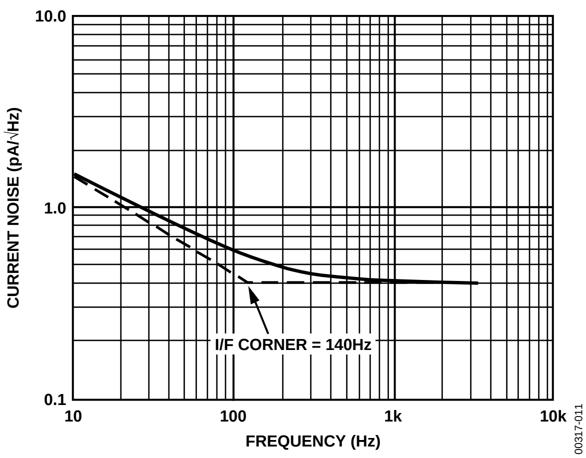

Figure 11. Current Noise Density vs. Frequency

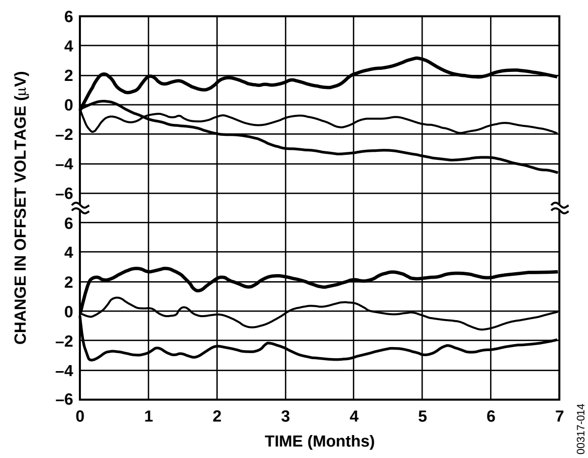

Figure 14. Long-Term Offset Voltage Drift of Six Representative Units

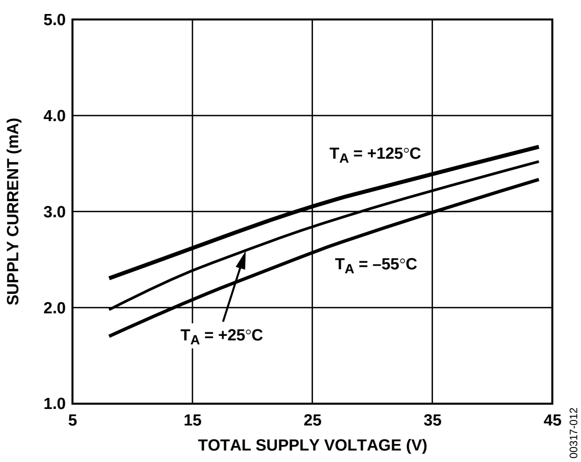

Figure 12. Supply Current vs. Supply Voltage

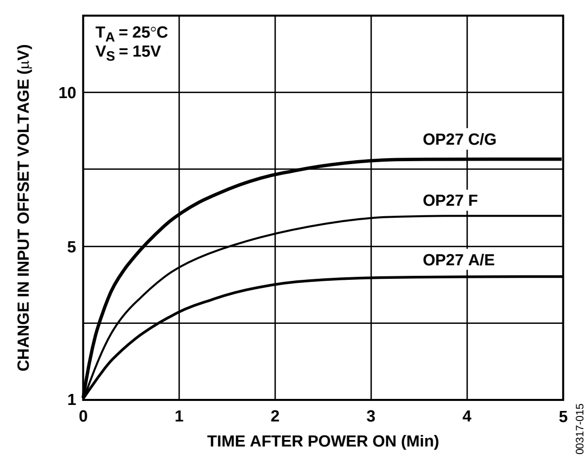

Figure 15. Warm-Up Offset Voltage Drift

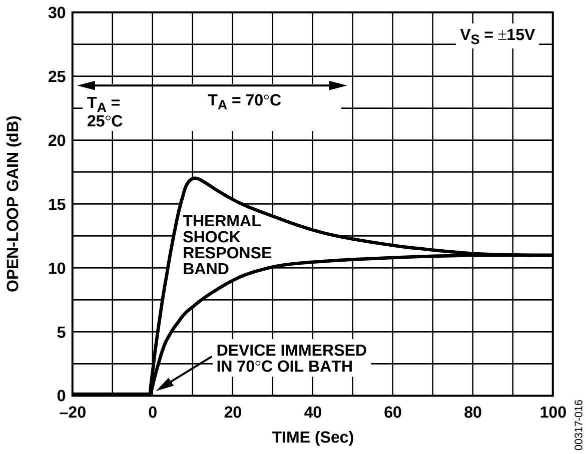

Figure 16. Offset Voltage Change Due to Thermal Shock

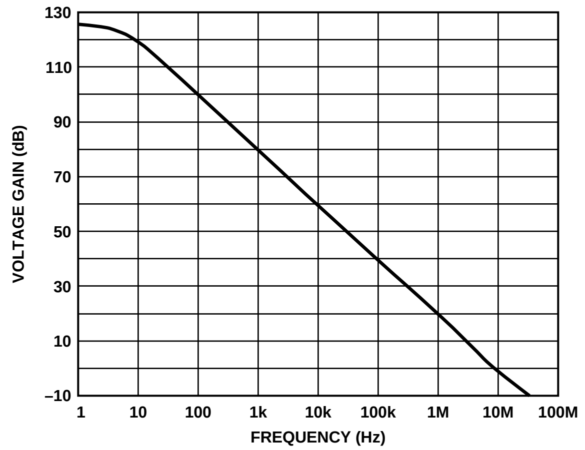

Figure 19. Open-Loop Gain vs. Frequency

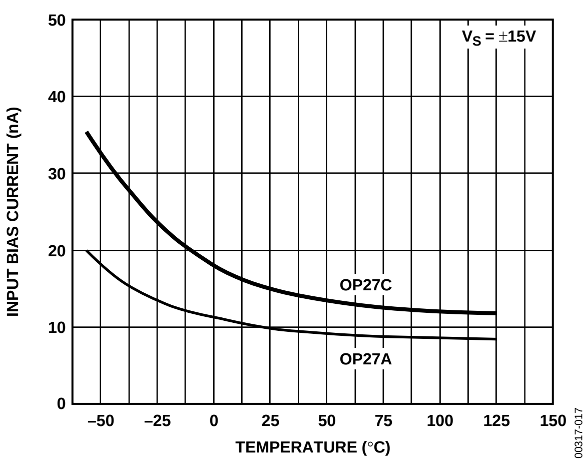

Figure 17. Input Bias Current vs. Temperature

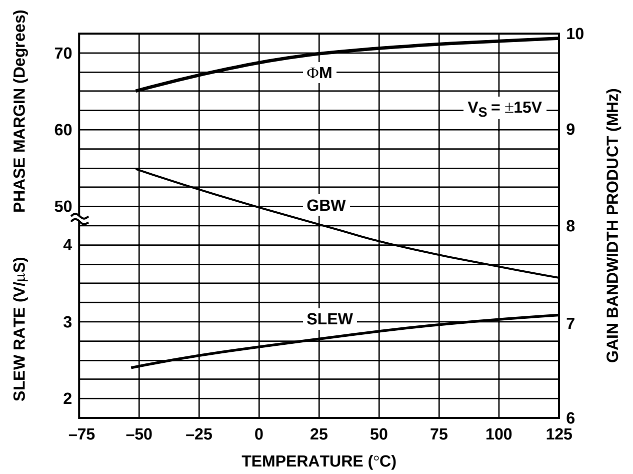

Figure 20. Slew Rate, Gain-Bandwidth Product, Phase Margin vs. Temperature

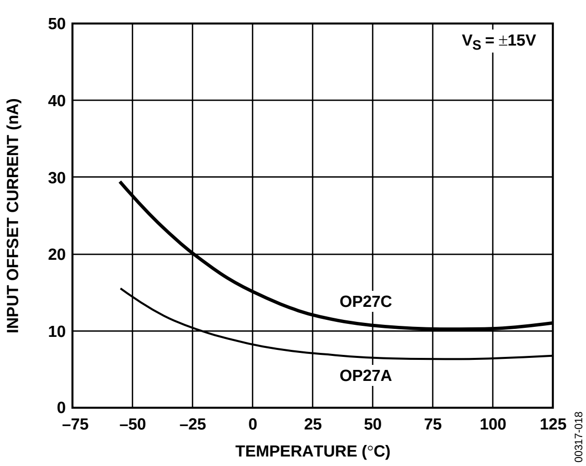

Figure 18. Input Offset Current vs. Temperature

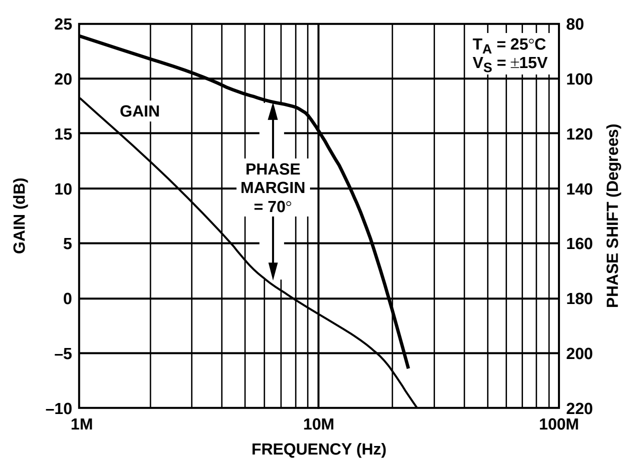

Figure 21. Gain, Phase Shift vs. Frequency

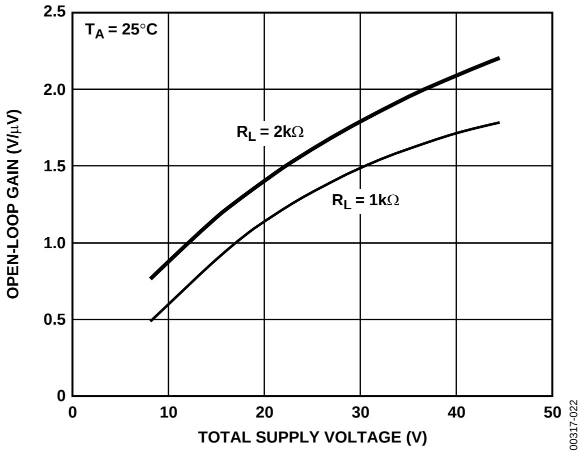

Figure 22. Open-Loop Voltage Gain vs. Supply Voltage

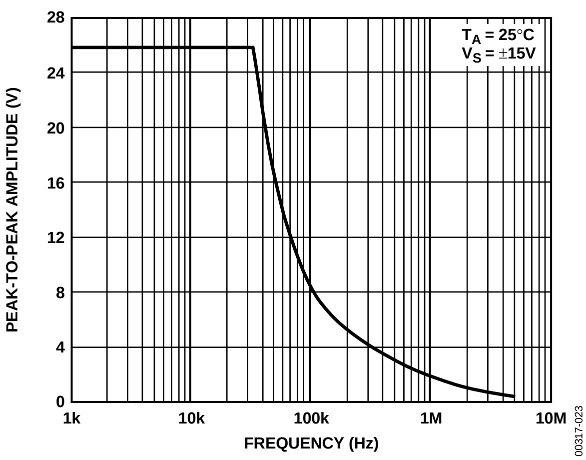

Figure 23. Maximum Output Swing vs. Frequency

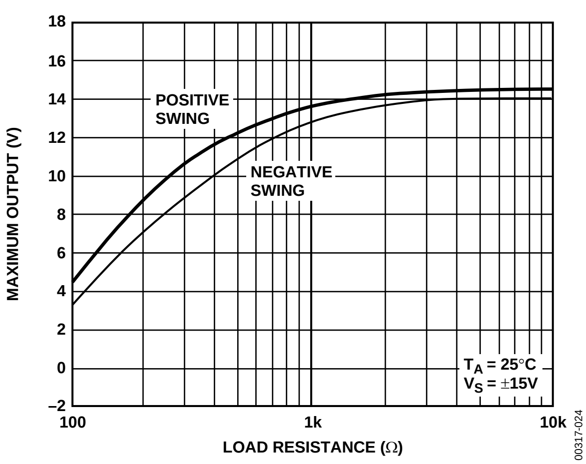

Figure 24. Maximum Output Voltage vs. Load Resistance

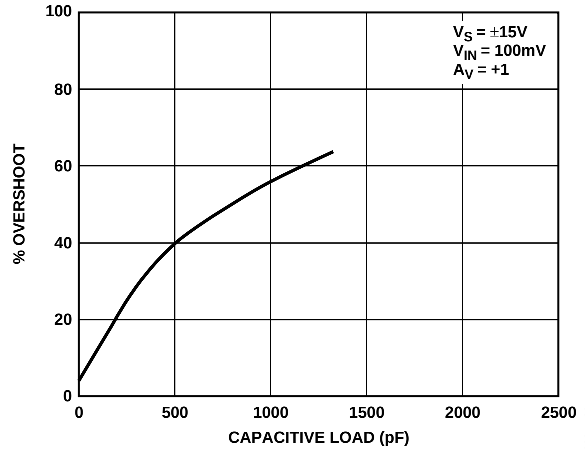

Figure 25. Small-Signal Overshoot vs. Capacitive Load

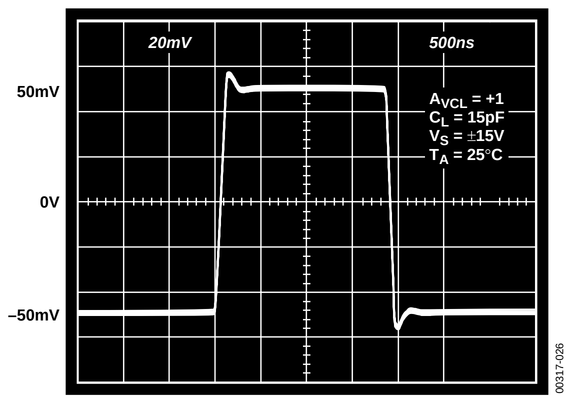

Figure 26. Small-Signal Transient Response

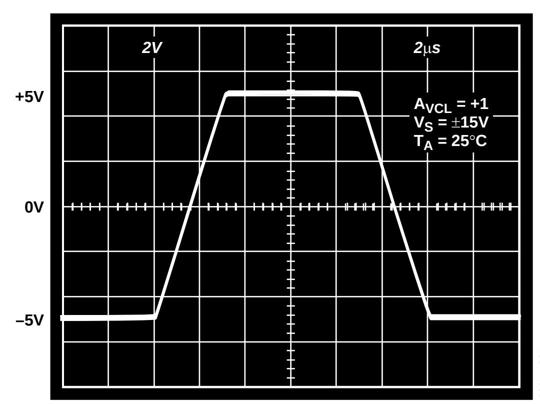

Figure 27. Large-Signal Transient Response

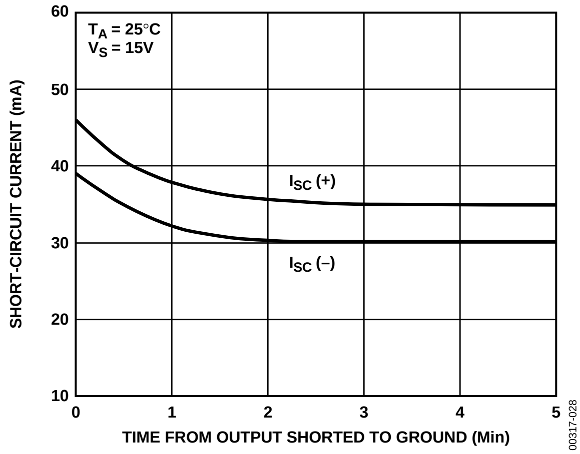

Figure 28. Short-Circuit Current vs. Time

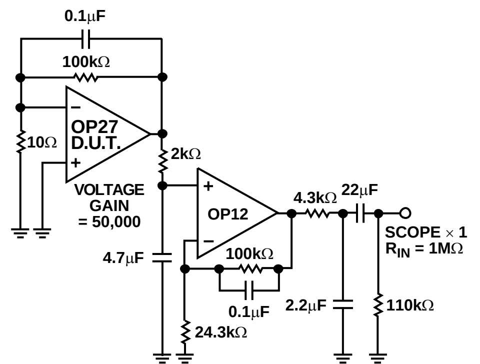

Figure 31. Voltage Noise Test Circuit (0.1 Hz to 10 Hz)

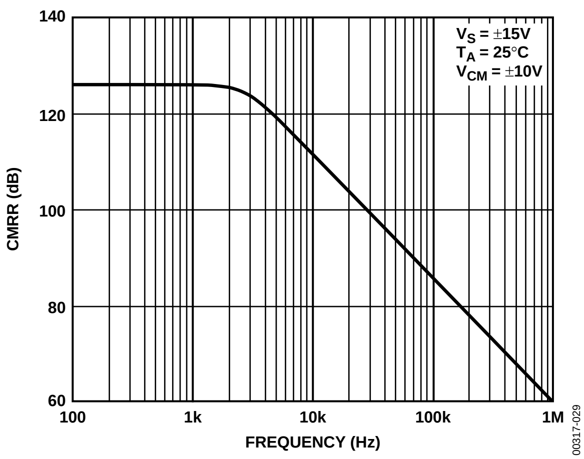

Figure 29. CMRR vs. Frequency

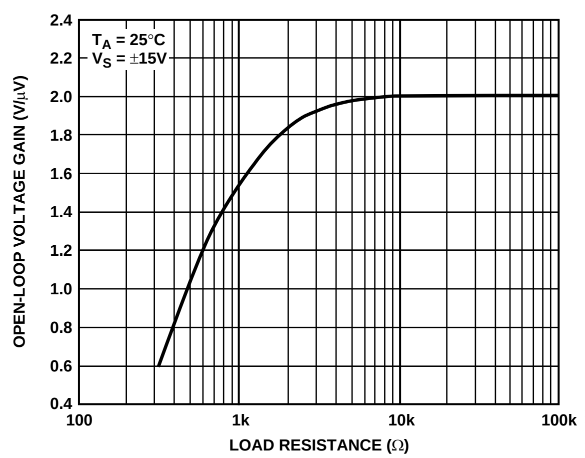

Figure 32. Open-Loop Voltage Gain vs. Load Resistance

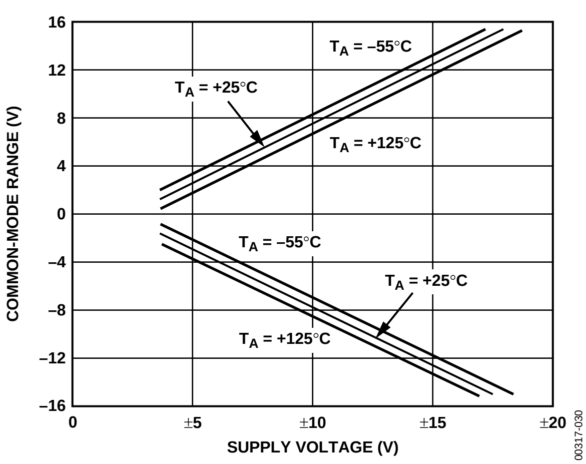

Figure 30. Common-Mode Input Range vs. Supply Voltage

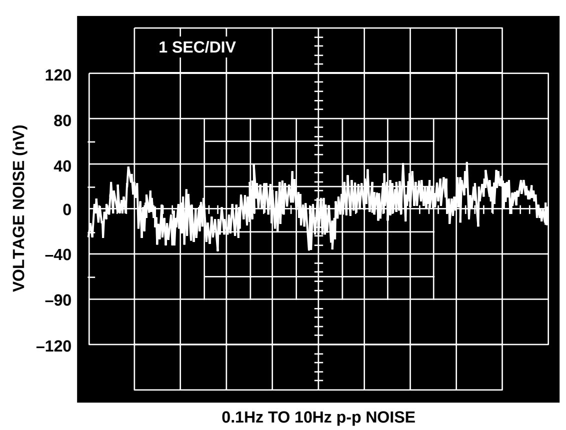

Figure 33. Low-Frequency Noise

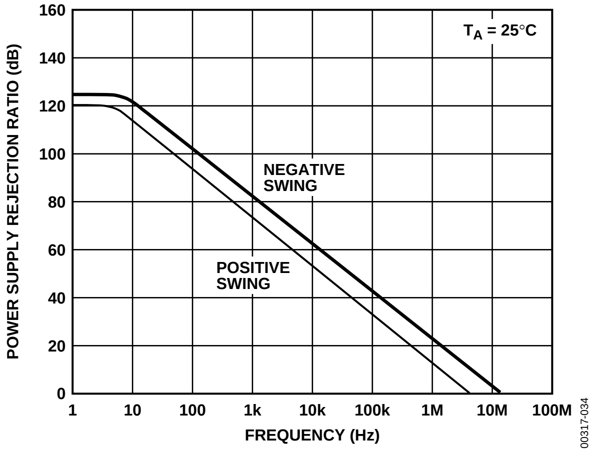

Figure 34. PSRR vs. Frequency

APPLICATION INFORMATION

OP27 series units may be inserted directly into 725 and OP07 sockets with or without removal of external compensation or nulling components. Additionally, the OP27 may be fitted to unnulled 741-type sockets; however, if conventional 741 nulling circuitry is in use, it should be modified or removed to ensure correct OP27 operation. OP27 offset voltage may be nulled to 0 (or another desired setting) using a potentiometer (see Figure 35).

The OP27 provides stable operation with load capacitances of up to 2000 pF and ±10 V swings; larger capacitances should be decoupled with a 50 Ω resistor inside the feedback loop. The OP27 is unity-gain stable.

Thermoelectric voltages generated by dissimilar metals at the input terminal contacts can degrade the drift performance. Best operation will be obtained when both input contacts are maintained at the same temperature.

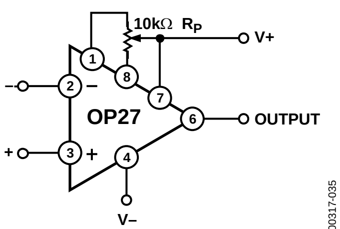

Figure 35. Offset Nulling Circuit

OFFSET VOLTAGE ADJUSTMENT

The input offset voltage of the OP27 is trimmed at wafer level. However, if further adjustment of V_{OS} is necessary, a 10 kΩ trim potentiometer can be used. TCV_{OS} is not degraded (see Figure 35). Other potentiometer values from 1 kΩ to 1 MΩ can be used with a slight degradation (0.1 μV/°C to 0.2 μV/°C) of TCV_{OS}. Trimming to a value other than zero creates a drift of approximately (V_{OS}/300) μV/°C. For example, the change in TCV_{OS} will be 0.33 μV/°C if V_{OS} is adjusted to 100 μV. The offset voltage adjustment range with a 10 kΩ potentiometer is ±4 mV. If smaller adjustment range is required, the nulling sensitivity can be reduced by using a smaller potentiometer in conjunction with fixed resistors. For example, Figure 36 shows a network that will have a 280 μV adjustment range.

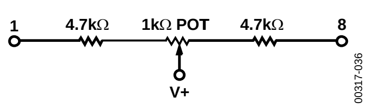

Figure 36. Offset Voltage Adjustment

NOISE MEASUREMENTS

To measure the 80 nV p-p noise specification of the OP27 in the 0.1 Hz to 10 Hz range, the following precautions must be observed:

- The device must be warmed up for at least five minutes. As shown in the warm-up drift curve, the offset voltage typically changes 4 μV due to increasing chip temperature after power-up. In the 10-second measurement interval, these temperature-induced effects can exceed tens-of-nanovolts.
- For similar reasons, the device has to be well-shielded from air currents. Shielding minimizes thermocouple effects.
- Sudden motion in the vicinity of the device can also feedthrough to increase the observed noise.
- The test time to measure 0.1 Hz to 10 Hz noise should not exceed 10 seconds. As shown in the noise-tester frequency response curve, the 0.1 Hz corner is defined by only one zero. The test time of 10 seconds acts as an additional zero to eliminate noise contributions from the frequency band below 0.1 Hz.
- A noise-voltage-density test is recommended when measuring noise on a large number of units. A 10 Hz noise-voltage-density measurement will correlate well with a 0.1 Hz to 10 Hz peak-to-peak noise reading, since both results are determined by the white noise and the location of the 1/f corner frequency.

UNITY-GAIN BUFFER APPLICATIONS

When $R_f \leq 100\ \Omega$ and the input is driven with a fast, large signal pulse (>1 V), the output waveform will look as shown in the pulsed operation diagram (Figure 37).

During the fast feedthrough-like portion of the output, the input protection diodes effectively short the output to the input, and a current, limited only by the output short-circuit protection, will be drawn by the signal generator. With $R_f \geq 500\ \Omega$, the output is capable of handling the current requirements ($I_L \leq 20$ mA at 10 V); the amplifier will stay in its active mode and a smooth transition will occur.

When $R_f > 2$ kΩ, a pole will be created with R_f and the amplifier's input capacitance (8 pF) that creates additional phase shift and reduces phase margin. A small capacitor (20 pF to 50 pF) in parallel with R_f will eliminate this problem.

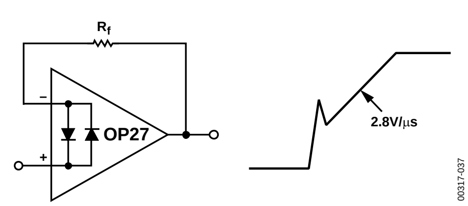

Figure 37. Pulsed Operation

COMMENTS ON NOISE

The OP27 is a very low-noise, monolithic op amp. The outstanding input voltage noise characteristics of the OP27 are achieved mainly by operating the input stage at a high quiescent current. The input bias and offset currents, which would normally increase, are held to reasonable values by the input bias-current cancellation circuit. The OP27A/E has I_B and I_{OS} of only ±40 nA and 35 nA at 25°C respectively. This is particularly important when the input has a high source resistance. In addition, many audio amplifier designers prefer to use direct coupling. The high I_B, V_{OS}, and TCV_{OS} of previous designs have made direct coupling difficult, if not impossible, to use.

Voltage noise is inversely proportional to the square root of bias current, but current noise is proportional to the square root of bias current. The OP27's noise advantage disappears when high source-resistors are used. Figure 38, Figure 39, Figure 40 compare OP27's observed total noise with the noise performance of other devices in different circuit applications.

$$Total\,Noise = \begin{bmatrix} (Voltage\,Noise)^2 + \\ (Current\,Noise \times R_S)^2 + \\ (Resistor\,Noise)^2 \end{bmatrix}^{1/2}$$

Figure 38 shows noise vs. source resistance at 1000 Hz. The same plot applies to wideband noise. To use this plot, multiply the vertical scale by the square root of the bandwidth.

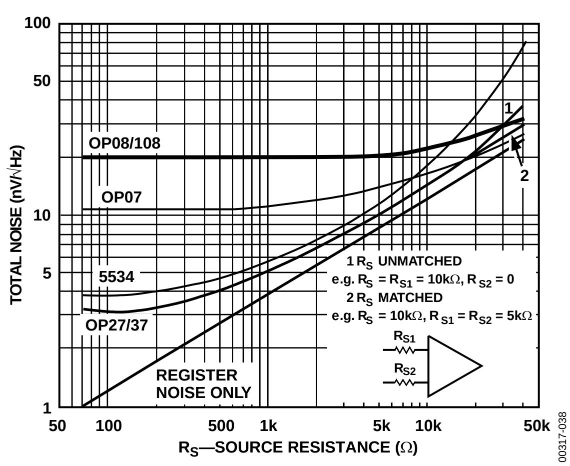

Figure 38. Noise vs. Source Resistance (Including Resistor Noise) at 1000 Hz

At R_S < 1 kΩ, the OP27's low voltage noise is maintained. With R_S < 1 kΩ, total noise increases but is dominated by the resistor noise rather than current or voltage noise. It is only beyond R_S of 20 kΩ that current noise starts to dominate. The argument can be made that current noise is not important for applications with low-to-moderate source resistances. The crossover between the OP27, OP07, and OP08 noise occurs in the 15 kΩ to 40 kΩ region.

Figure 39 shows the 0.1 Hz to 10 Hz peak-to-peak noise. Here the picture is less favorable; resistor noise is negligible and current noise becomes important because it is inversely proportional to the square root of frequency. The crossover with the OP07 occurs in the 3 kΩ to 5 kΩ range depending on whether balanced or unbalanced source resistors are used (at 3 kΩ the I_B and I_{OS} error also can be 3× the V_{OS} spec.).

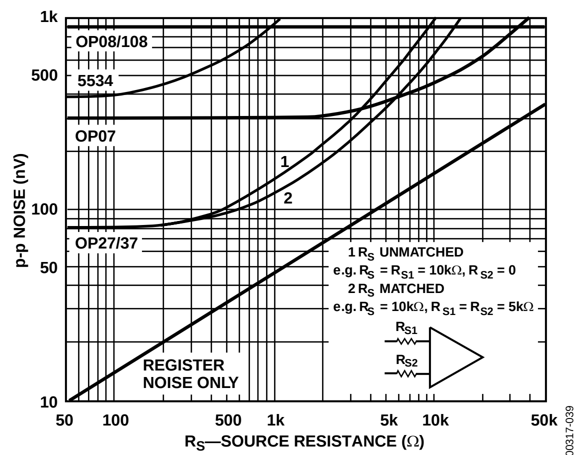

Figure 39. Peak-to-Peak Noise (0.1 Hz to 10 Hz) as Source Resistance (Includes Resistor Noise)

Therefore, for low frequency applications, the OP07 is better than the OP27/OP37 when RS > 3 kΩ. The only exception is when gain error is important.

Figure 40 illustrates the 10 Hz noise. As expected, the results are between the previous two figures.

For reference, typical source resistances of some signal sources are listed in Table 7.

Table 7.

Device	Source Impedance	Comments
Strain Gauge	<500 Ω	Typically used in low-frequency applications.
Magnetic Tapehead	<1500 Ω	Low is very important to reduce self-magnetization problems when direct coupling is used. OP27 IB can be neglected.
Magnetic Phonograph Cartridges	<1500 Ω	Similar need for low IB in direct coupled applications. OP27 will not introduce any self-magnetization problem.
Linear Variable Differential Transformer	<1500 Ω	Used in rugged servo-feedback applications. Bandwidth of interest is 400 Hz to 5 kHz.

Table 8. Open-Loop Gain

Frequency at	OP07	OP27	OP37
3 Hz	100 dB	124 dB	125 dB
10 Hz	100 dB	120 dB	125 dB
30 Hz	90 dB	110 dB	124 dB

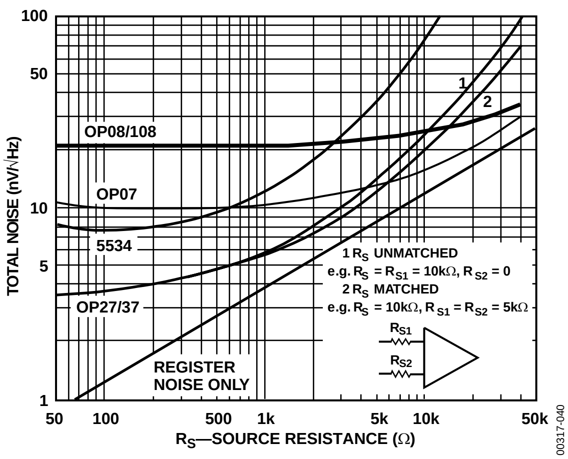

Figure 40. 10 Hz Noise vs. Source Resistance (Includes Resistor Noise) Audio Applications

AUDIO APPLICATIONS

The following applications information has been abstracted from a PMI article in the 12/20/80 issue of Electronic Design magazine and updated.

Figure 41 is an example of a phono pre-amplifier circuit using the OP27 for A1; R1-R2-C1-C2 form a very accurate RIAA network with standard component values. The popular method to accomplish RIAA phono equalization is to employ frequency-dependent feedback around a high quality gain block. Properly chosen, an RC network can provide the three necessary time constants of 3180, 318, and 75 μs.

For initial equalization accuracy and stability, precision metal film resistors and film capacitors of polystyrene or polypropylene are recommended because they have low voltage coefficients, dissipation factors, and dielectric absorption. (High-K ceramic capacitors should be avoided here, though low-K ceramics—such as NPO types, which have excellent dissipation factors and somewhat lower dielectric absorption—can be considered for small values.)

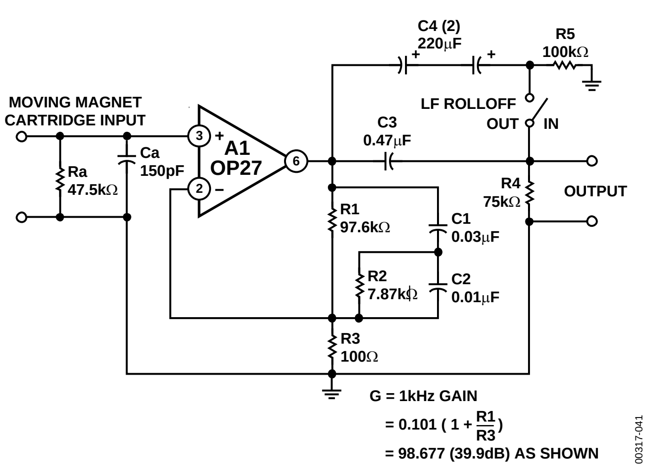

Figure 41. Phono Preamplifier Circuit

The OP27 brings a 3.2 nV/√Hz voltage noise and 0.45 pA/√Hz current noise to this circuit. To minimize noise from other sources, R3 is set to a value of 100 Ω, which generates a voltage noise of 1.3 nV/√Hz. The noise increases the 3.2 nV/√Hz of the amplifier by only 0.7 dB. With a 1 kΩ source, the circuit noise measures 63 dB below a 1 mV reference level, unweighted, in a 20 kHz noise bandwidth.

Gain (*G*) of the circuit at 1 kHz can be calculated by the expression:

$$G = 0.101\left(1 + \frac{R1}{R3}\right)$$

For the values shown, the gain is just under 100 (or 40 dB). Lower gains can be accommodated by increasing R3, but gains higher than 40 dB will show more equalization errors because of the 8 MHz gain-bandwidth of the OP27.

This circuit is capable of very low distortion over its entire range, generally below 0.01% at levels up to 7 V rms. At 3 V output levels, it will produce less than 0.03% total harmonic distortion at frequencies up to 20 kHz.

Capacitor C3 and Resistor R4 form a simple −6 dB-per-octave rumble filter, with a corner at 22 Hz. As an option, the switch-selected Shunt Capacitor C4, a nonpolarized electrolytic, bypasses the low-frequency roll-off. Placing the rumble filter's high-pass action after the preamp has the desirable result of discriminating against the RIAA-amplified low frequency noise components and pickup-produced low frequency disturbances.

A preamplifier for NAB tape playback is similar to an RIAA phono preamp, though more gain is typically demanded, along with equalization requiring a heavy low frequency boost. The circuit in Figure 41 can be readily modified for tape use, as shown by Figure 42.

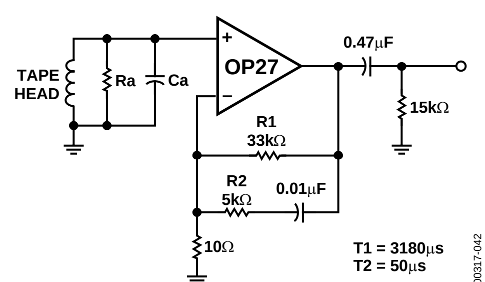

Figure 42. Tape-Head Preamplifier

While the tape-equalization requirement has a flat high frequency gain above 3 kHz (T2 = 50 μs), the amplifier need not be stabilized for unity gain. The decompensated OP37 provides a greater bandwidth and slew rate. For many applications, the idealized time constants shown may require trimming of R1 and R2 to optimize frequency response for nonideal tape-head performance and other factors (see the References section).

The network values of the configuration yield a 50 dB gain at 1 kHz, and the dc gain is greater than 70 dB. Thus, the worst-case output offset is just over 500 mV. A single 0.47 μF output capacitor can block this level without affecting the dynamic range.

The tapehead can be coupled directly to the amplifier input, because the worst-case bias current of 80 nA with a 400 mH, 100 μ inch head (such as the PRB2H7K) will not be troublesome.

One potential tapehead problem is presented by amplifier bias-current transients that can magnetize a head. The OP27 and OP37 are free of bias-current transients upon power-up or power-down. However, it is always advantageous to control the speed of power-supply rise and fall, to eliminate transients.

In addition, the dc resistance of the head should be carefully controlled and preferably below 1 kΩ. For this configuration, the bias-current-induced offset voltage can be greater than the 100 pV maximum offset if the head resistance is not sufficiently controlled.

A simple, but effective, fixed-gain transformerless microphone preamp (Figure 43) amplifies differential signals from low impedance microphones by 50 dB and has an input impedance of 2 kΩ. Because of the high working gain of the circuit, an OP37 helps to preserve bandwidth, which will be 110 kHz. As the OP37 is a decompensated device (minimum stable gain of 5), a dummy resistor, R_P, may be necessary if the microphone is to be unplugged. Otherwise, the 100% feedback from the open input may cause the amplifier to oscillate.

Common-mode input-noise rejection will depend upon the match of the bridge-resistor ratios. Either close-tolerance (0.1%) types should be used, or R4 should be trimmed for best CMRR. All resistors should be metal film types for best stability and low noise.

Noise performance of this circuit is limited more by the Input Resistors R1 and R2 than by the op amp, as R1 and R2 each generate a 4 nV/√Hz noise, while the op amp generates a 3.2 nV/√Hz noise. The rms sum of these predominant noise sources will be about 6 nV/√Hz, equivalent to 0.9 μV in a 20 kHz noise bandwidth, or nearly 61 dB below a 1 mV input signal. Measurements confirm this predicted performance.

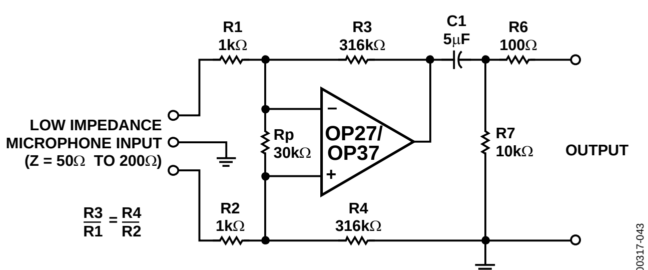

Figure 43. Fixed Gain Transformerless Microphone Preamplifier

For applications demanding appreciably lower noise, a high quality microphone transformer-coupled preamp (Figure 44) incorporates the internally compensated OP27. T1 is a JE-115K-E 150 Ω/15 kΩ transformer that provides an optimum source resistance for the OP27 device. The circuit has an overall gain of 40 dB, the product of the transformer's voltage setup and the op amp's voltage gain.

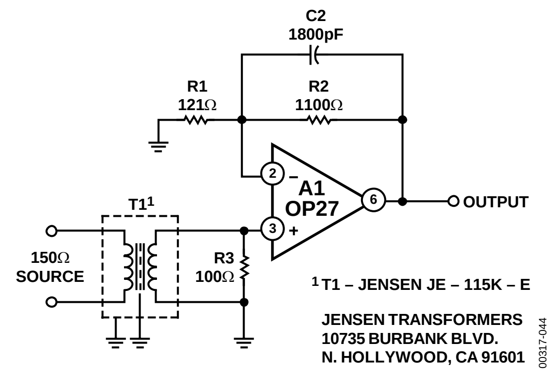

Figure 44. High Quality Microphone Transformer Coupled Preamplifier

Gain may be trimmed to other levels, if desired, by adjusting R2 or R1. Because of the low offset voltage of the OP27, the output offset of this circuit will be very low, 1.7 mV or less, for a 40 dB gain. The typical output blocking capacitor can be eliminated in such cases, but it is desirable for higher gains to eliminate switching transients.

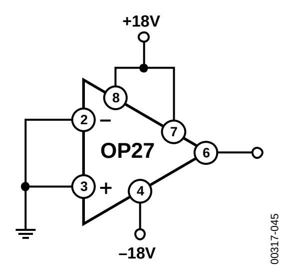

Figure 45. Burn-In Circuit

Capacitor C2 and Resistor R2 form a 2 μs time constant in this circuit, as recommended for optimum transient response by the transformer manufacturer. With C2 in use, A1 must have unity-gain stability. For situations where the 2 μs time constant is not necessary, C2 can be deleted, allowing the faster OP37 to be employed.

Some comment on noise is appropriate to understand the capability of this circuit. A 150 Ω resistor and R1 and R2 gain resistors connected to a noiseless amplifier will generate 220 nV of noise in a 20 kHz bandwidth, or 73 dB below a 1 mV reference level. Any practical amplifier can only approach this noise level; it can never exceed it. With the OP27 and T1 specified, the additional noise degradation will be close to 3.6 dB (or −69.5 referenced to 1 mV).

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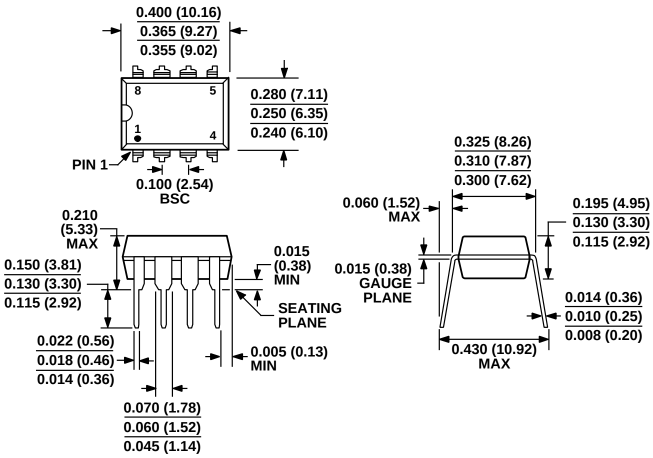
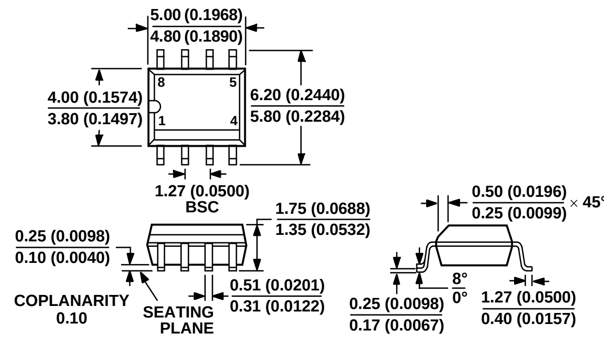
OUTLINE DIMENSIONS



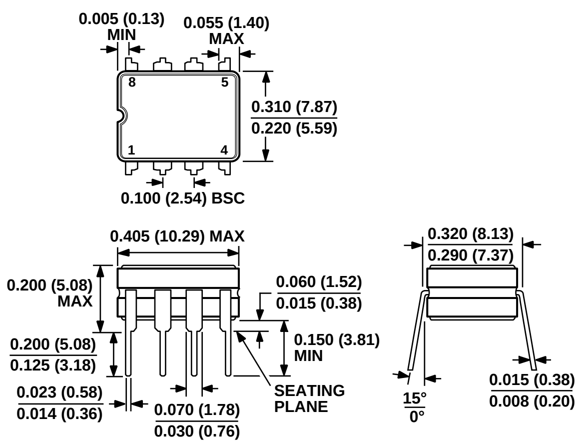
COMPLIANT TO JEDEC STANDARDS MS-001-BA
CONTROLLING DIMENSIONS ARE IN INCHES; MILLIMETER DIMENSIONS (IN PARENTHESES) ARE ROUNDED-OFF INCH EQUIVALENTS FOR REFERENCE ONLY AND ARE NOT APPROPRIATE FOR USE IN DESIGN.
CORNER LEADS MAY BE CONFIGURED AS WHOLE OR HALF LEADS.

Figure 46. 8-Lead Plastic Dual-in-Line Package [PDIP]
(N-8)
P-Suffix
Dimensions shown in inches and (millimeters)



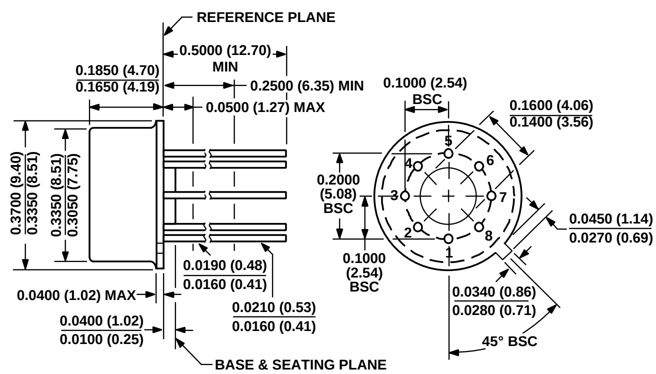
COMPLIANT TO JEDEC STANDARDS MS-012-AA
CONTROLLING DIMENSIONS ARE IN MILLIMETERS; INCH DIMENSIONS (IN PARENTHESES) ARE ROUNDED-OFF MILLIMETER EQUIVALENTS FOR REFERENCE ONLY AND ARE NOT APPROPRIATE FOR USE IN DESIGN.

Figure 48. 8-Lead Standard Small Outline Package [SOIC]
Narrow Body
(R-8)
S-Suffix
Dimensions shown in millimeters and (inches)



CONTROLLING DIMENSIONS ARE IN INCHES; MILLIMETER DIMENSIONS (IN PARENTHESES) ARE ROUNDED-OFF INCH EQUIVALENTS FOR REFERENCE ONLY AND ARE NOT APPROPRIATE FOR USE IN DESIGN.

Figure 47. 8-Lead Ceramic DIP – Glass Hermetic Seal [CERDIP]
(Q-8)
Z-Suffix
Dimensions shown in inches and (millimeters)



COMPLIANT TO JEDEC STANDARDS MO-002-AK
CONTROLLING DIMENSIONS ARE IN INCHES; MILLIMETER DIMENSIONS (IN PARENTHESES) ARE ROUNDED-OFF INCH EQUIVALENTS FOR REFERENCE ONLY AND ARE NOT APPROPRIATE FOR USE IN DESIGN.

Figure 49. 8-Lead Metal Can [TO-99]
(H-08)
J-Suffix
Dimensions shown in inches and (millimeters)

ORDERING GUIDE

Model	Temperature Range	Package Description	Package Option
OP27AJ/883C	–55° to +125°C	8-Lead Metal Can (TO-99)	J-Suffix (H-08)
OP27GJ	–40° to +85°C	8-Lead Metal Can (TO-99)	J-Suffix (H-08)
OP27AZ	–55° to +125°C	8-Lead CERDIP	Z-Suffix (Q-8)
OP27AZ/883C	–55° to +125°C	8-Lead CERDIP	Z-Suffix (Q-8)
OP27EZ	–25° to +85°C	8-Lead CERDIP	Z-Suffix (Q-8)
OP27GZ	–40° to +85°C	8-Lead CERDIP	Z-Suffix (Q-8)
OP27EP	–25° to +85°C	8-Lead PDIP	P-Suffix (N-8)
OP27EPZ[1]	–25° to +85°C	8-Lead PDIP	P-Suffix (N-8)
OP27GP	–40° to +85°C	8-Lead PDIP	P-Suffix (N-8)
OP27GPZ[1]	–40° to +85°C	8-Lead PDIP	P-Suffix (N-8)
OP27GS	–40° to +85°C	8-Lead SOIC	S-Suffix (R-8)
OP27GS-REEL	–40° to +85°C	8-Lead SOIC	S-Suffix (R-8)
OP27GS-REEL7	–40° to +85°C	8-Lead SOIC	S-Suffix (R-8)
OP27GSZ[1]	–40° to +85°C	8-Lead SOIC	S-Suffix (R-8)
OP27GSZ-REEL[1]	–40° to +85°C	8-Lead SOIC	S-Suffix (R-8)
OP27GSZ-REEL7[1]	–40° to +85°C	8-Lead SOIC	S-Suffix (R-8)
OP27NBC		Die	

[1] Z = Pb-free part.

D00317-0-12/05(E)